Dual Monolithic Tone Decoder

GENERAL DESCRIPTION

The XR-2567 is a dual monolithic tone decoder of the 567-type that is ideally suited for tone or frequency decoding in multiple-tone communication systems. Each decoder of the XR-2567 can be used independently or both sections can be interconnected for dual operation. The matching and temperature tracking characteristics between decoders on this monolithic chip are superior to those available from two separate tone decoder packages.

The XR-2567 operates over a frequency range of 0.01Hz to 500kHz. Supply voltages can vary from 4.5V to 12V, with internal voltage regulation provided for supplies between 7V and 12V. Each decoder consists of a phase-locked loop (PLL), a quadrature AM detector, a voltage comparator, and a logic compatible output that can sink more than 100mA of load current.

The center frequency of each decoder is set by an external resistor and capacitor which determine the free-running frequency of each PLL. When an input tone is present within the passband of the circuit, the PLL "locks" on the input signal. The logic output, which is normally "high", then switches to a "low" state during this "lock" condition.

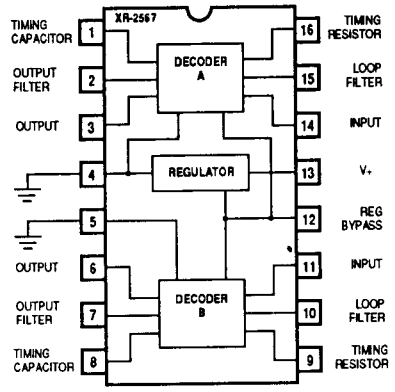
FEATURES

Replaces two 567-type decoders
Excellent temperature tracking between decoders
Bandwidth adjustable from 0 to 14%
Logic compatible outputs with 100mA sink capability
Center frequency matching (1% typ.)
Center frequency adjustable from 0.01Hz to 500kHz
Inherent immunity to false triggering
Frequency range adjustable over 20:1 range by external resistor.

APPLICATIONS

Touch-Tone® Decoding
Sequential Tone Decoding
Dual-Tone Decoding/Encoding
Communications Paging
Ultrasonic Remote-Control and Monitoring
Full-Duplex Carrier-Tone Transceiver
Wireless Intercom
Dual Precision Oscillator
FSK Generation and Detection

PIN ASSIGNMENT



ABSOLUTE MAXIMUM RATINGS

Power Supply	
with Internal Regulator	14V
without Regulator (Pins 12 and 13 shorted)	10V
Power Dissipation	
Ceramic Package	750mW
Derate Above +25°C	6mW/°C
Plastic Package	625mW/°C
Derate Above +25°C	5.5mW/°C
Storage Temperature	–65°C to +150°C

ORDERING INFORMATION

Part Number	Package	Operating Temperature
XR-2567M	Ceramic	–55°C to + 125°C
XR-2567CN	Ceramic	0°C to + 70°C
XR-2567CP	Plastic	0°C to + 70°C

ELECTRICAL CHARACTERISTICS

Test Conditions: V_{CC} = +5V. T_A = 25°C, unless otherwise specified. Test circuit of Figure 2, S_1 closed unless otherwise specified.

PARAMETERS	LIMITS MIN	LIMITS TYP	LIMITS MAX	UNITS	CONDITIONS
GENERAL					
Supply Voltage Range					
Without Regulator	4.75		7	V_{dc}	See Figure 5, S_1 closed.
With Internal Regulator	6.5		12	V_{dc}	See Figure 5, S_1 open.
Supply Current (both decoders)					See Figure 7,8
Quiescent XR-2567M		12	16	mA	R_L = 20 kΩ
XR-2567C		14	20	mA	R_L = 20 kΩ
Activated XR-2567M		22	26	mA	R_L = 20 kΩ
XR-2567C		24	30	mA	R_L = 20 kΩ
Output Voltage			15	V	
Negative Voltage at Input			-10	V	
Positive Voltage at Input			V_{CC} + 0.5	V	
CENTER FREQUENCY (each decoder section)					
Highest Center Frequency	100	500		kHz	
Center Frequency Stability					
Temperature T_A = 25°C		35		ppm/°C	See Figure 14
0°C < T_T < 70°C *		±60		ppm/°C	See Figure 14
-55°C < T_T < +125°C*		±140		ppm/°C	See Figure 14
Supply Voltage					
Without Regulator					
XR-2567M		0.5	1.0	%/V	f_o = 100kHz
XR-2567C		0.7	2.0	%/V	f_o = 100kHz
With Internal Regulator					
XR-2567M		0.05		%/V	f_o = 100kHz, V_{CC} = 9V
XR-2567C		0.1		%/V	f_o = 100kHz, V_{CC} = 9V
DETECTION BANDWIDTH (each decoder section)					
Largest Detection Bandwidth					
XR-2567M	12	14	16	% of f_o	f_o = 100kHz
XR-2567C	10	14	18	% of f_o	f_o = 100kHz
Largest Detection Bandwidth Skew					
XR-2567M		1	2	% of f_o	
XR-2567C		1	3	% of f_o	
Largest Detection Bandwidth Variation					
Temperature		±0.1		% /°C	V_{IN} = 300mV rms
Supply Voltage		±2		%/V	V_{IN} = 300mV rms
INPUT (each decoder section)					
Input Resistance		20		kΩ	
Smallest Detectable Input Voltage		20	25	mV rms	I_L = 100mA, f_i = f_o
Largest No-Output Input Voltage	10	15		mV rms	I_L = 100mA, f_i = f_o
Greatest Simultaneous Outband Signal to Inband Signal Ratio		+6		dB	
Minimum Input Signal to Wideband Noise Ratio		-6		dB	Noise BW = 140kHz
OUTPUT (each decoder section)					
Output Saturation Voltage		0.2	0.4	V	I_L = 30mA, V_{IN} = 25mV rms
		0.6	1.0	V	I_L = 100mA, V_{IN} = 25mV rms
Output Leakage Current		0.01	25	µA	
Fastest ON-OFF Cycling Rate		f_o/20			
Output Rise Time		150		ns	R_L = 50Ω
Output Fall Time		30		ns	R_L = 50Ω
MATCHING CHARACTERISTICS					
Center Frequency Matching		1		%	f_o = 10kHz
Temperature Drift Matching		±20		ppm/°C	0°C < T_A < 70°C
		±50		ppm/°C	-55°C < T_A < 125°C

*These parameters, although guaranteed over the recommended operating conditions, are not 100% tested in production.

SYSTEM DESCRIPTION

The XR-2567 dual monolithic tone decoder consists of two independant 567-type circuits and an on board voltage regulator. Each decoder has a phase detector, low pass filter, and current controlled oscillator which comprise the basic phase locked loop, plus an additional low pass filter and quadrature detector enabling detection of in-band signals. Both devices have normally high open collector outputs capable of sinking 100mA.

The input signal is applied to Pin 14 (device A) or Pin 11 (device B), both with 20kΩ nominal input resistance. Free running frequency is controlled by an RC network at Pins 1 and 16 (device A) or Pins 8 and 9 (device B). A capacitor on Pin 2 (A), or Pin 7 (B) serves as the output filter and eliminates out-of-band triggering. PLL filtering is accomplished with a capacitor on Pin 15 (A), or Pin 10 (B); bandwidth and skew are also dependant upon the circuitry here. Bandwidth is adjustable from 0% to 14% of the center frequency. Pin 13 is $+V_{CC}$ (4.75 to 12V nominal, 14V maximum); Pin 7 is ground; and Pin 3 (A) or Pin 6 (B) is the open collector output, pulling low when an in-band signal triggers the device.

The internal regulator needs to be bypassed for supply voltages below 7V. This is done by shorting Pin 12 to VCC. Supply voltages to Pin 12 which are over 7V need a bypass capacitor (1nF) to ground (see figure 2).

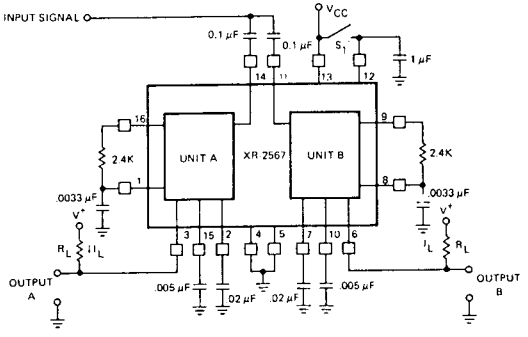
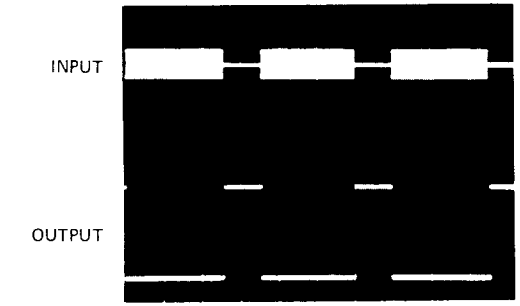


Figure 2. Test Circuit



Response to 100 mV rms tone burst
R_L = 100 ohms.

Figure 3. XR-2567 Typical Response

DEFINITIONS OF XR-2567 PARAMETERS

f_o is the *free-running frequency* of the current-controlled oscillator of the PLL with no input signal. It is determined by resistor R_1 and capacitor C_1; f_o can be approximated by

$$f_0 \approx \frac{1}{R_1 C_1} \text{ Hz}$$

where R_1 is in ohms and C_1 is in farads.

The detection bandwidth is the frequency range centered about f_o, within which an input signal larger than the threshold voltage (typically 20mV rms) will cause a "logic zero" state at the output. The detection bandwidth corresponds to the capture range of the PLL and is determined by the low-pass bandwidth filter. The bandwidth of the filter, as a percent of f_o, can be determined by the approximation

$$BW = 1070 \sqrt{\frac{V_i}{f_0 C_2}}$$

where V_i is the input signal in volts, rms, and C_2 is the capacitance in µF at Pins 10 or 15.

The largest detection bandwidth is the largest frequency range within which an input signal above the threshold voltage will cause a logical zero state at the output. The maximum detection bandwidth corresponds to the lock range of the PLL.

The detection band skew is a measure of how accurately the largest detection band is centered about the center frequency, f_o. It is defined as $(f_{max} + f_{min} - 2f_o)/f_o$, where f_{max} and f_{min} are the frequencies corresponding to the edges of the detection band. If necessary, the detection band skew can be reduced to zero by an optional centering adjustment. (See Optional Controls.)

DESCRIPTION OF CIRCUIT CONTROLS

Input (Pins 11 and 14)

The input signal is applied to Pins 14 and/or 11 through a coupling capacitor, C_C. These terminals are internally biased at a dc level 2 volts above ground and they have an input impedance level of approximately 20kΩ.

Timing Resistor R_1 and Capacitor C_1 (Pins 1, 8, 9, and 16)

The center frequency, f_o, of each decoder section is set by a resistor R_1 and a capacitor C_1. R_{1A} is connected between Pins 1 and 16 in decoder section A, and R_{1B} between Pins 8 and 9 of decoder section B. C_{1A} is connected from Pin 1 to ground, and C_{1B} from Pin 8 to ground, as shown in Figure 4. R_1 and C_1 should be selected for the desired center frequency by the expression $f_o \approx 1/R_1C_1$. For optimum temperature stability, R_1 should be selected such that $2k\Omega \leq R_1 \leq 20k\Omega$, and the R_1C_1 product should have sufficient stability over the projected operating temperature range.

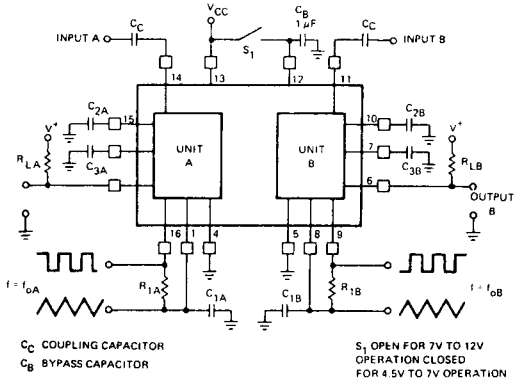


Figure 4. Circuit Connection Diagram

For decoder section A, the oscillator output can be obtained at either Pin 1 or 16. Pin 16 is the oscillator squarewave output which has a magnitude of approximately $V_{CC} - 1.4V$ and an average dc level of $V_{CC}/2$. A 1kΩ load may be driven from this point. The voltage at pin 1 is an exponential triangle waveform with a peak-to-peak amplitude of 1 volt and an average dc level of $V_{CC}/2$. Only high impedance loads should be connected to Pin 1 to avoid disturbing the temperature stability or duty cycle of the oscillator. For section B, Pin 9 is the squarewave output and Pin 8 the exponential triangle waveform output.

Loop Filter, C_2 (Pins 10 and 15)

Capacitors C_{2A} and C_{2B} connected from Pins 15 and 10 to ground are the single-pole, low-pass filters for the PLL portion of decoder sections A and B. The filter time constant is given by $T_2 = R_2C_2$, where R_2 (10kΩ) is the impedance at Pins 10 or 15. The selection of C_2 is determined by the detection bandwidth requirements and input signal amplitude as shown in Figures 10 and 12. One approach is to select an area of operation from the graph and then adjust the input level and value of C_2 accordingly. Or, if the input amplitude variation is known, the required f_oC_2 product can be found to give the desired bandwidth. Constant bandwidth operation requires $V_i >$ 200mV rms. Then, as noted in Figure 10, bandwidth will be controlled solely by the f_oC_2 product. (For additional information, see Optional Controls Section, "Speed of Response" and "Bandwidth Reduction".)

Pins 10 and 15 correspond to the PLL phase detector outputs of sections A and B, respectively. The voltage level at these pins is a linear function of frequency over the range of 0.95 to 1.05 f_o, with a slope of approximately 20mV/% frequency deviation.

Output Filter, C_3 (Pins 2 and 7)

Capacitors C_{3A} and C_{3B} connected from Pins 2 and 7 to ground form low-pass post detection filters for sections A and B respectively. The function of the post detection filter is to eliminate spurious outputs caused by out-of-band signals. The time constant of the filter can be expressed as $T_3 = R_3C_3$, where R_3 (4.7k) is the internal impedance at Pins 2 or 7.

TYPICAL CHARACTERISTICS

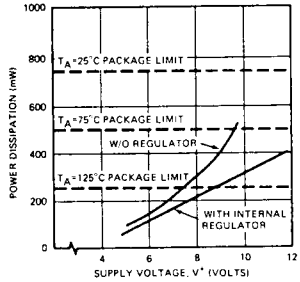


Figure 5. Internal Power Dissipation vs. Supply Voltage. Both Units Activated, R_L = 20 k

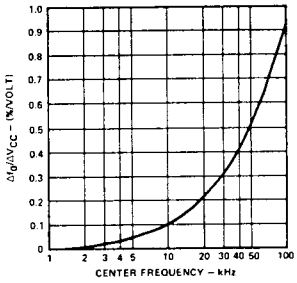


Figure 6. Power Supply Dependence of Center Frequency

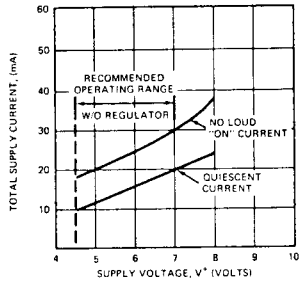


Figure 7. Total Supply Current vs. Supply Voltage for Operation without Internal Regulator (Pins 12 and 13 Shorted)

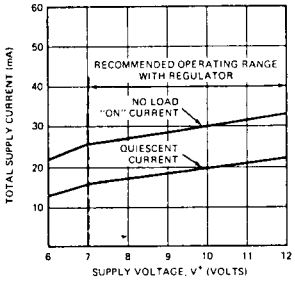


Figure 8. Total Supply Current vs. Supply Voltage for Operation with Internal Regulator (Pins 12 and 13 Not Connected)

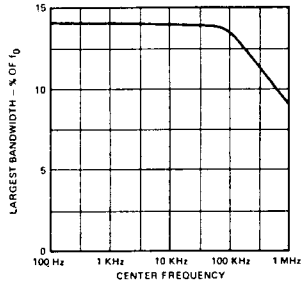


Figure 9. Largest Detection Bandwidth

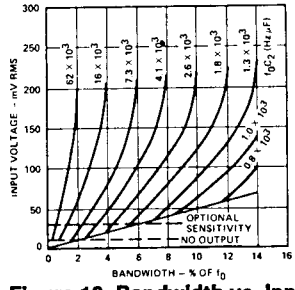


Figure 10. Bandwidth vs. Input Signal Amplitude (C_2 In μF)

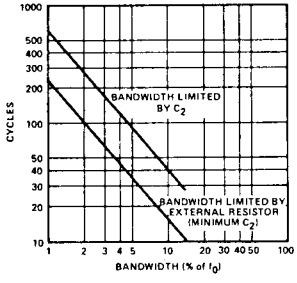


Figure 11. Greatest Number of Cycles Before Output

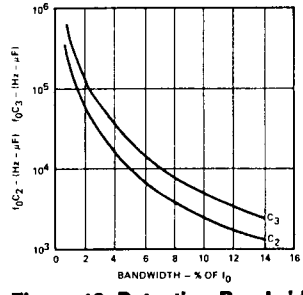


Figure 12. Detection Bandwidth as a Function of C_2 and C_3

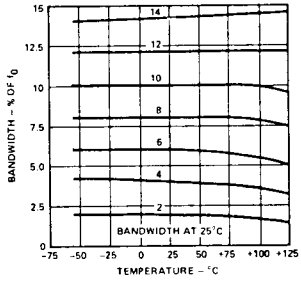


Figure 13. Bandwidth Variation with Temperature

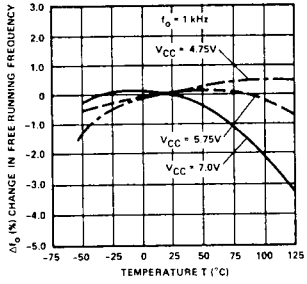


Figure 14. Frequency Drift with Temperature

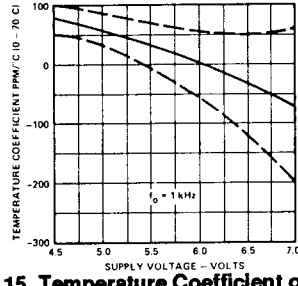


Figure 15. Temperature Coefficient of Center Frequency (Mean and S.D.)

The precise value of C_3 is not critical for most applications. To eliminate the possibility of false triggering by spurious signals, a minimum value for C_3 is $2C_2$, where C_2 is the loop filter capacitance for the corresponding decoder section. If C_3 is smaller than $2C_2$, then frequencies adjacent to the detection band may switch the output stage "off" and "on" at the beat frequency, or the output may pulse "off" and "on" during the turn- on transient.

If the value of C_3 becomes too large, the turn-on or turn-off time of the output stage will be delayed until the voltage change across C_3 reaches the threshold voltage. In certain applications, this delay may be desirable as a means of suppressing spurious outputs. (For additional information, see Optional Controls Section, "Speed of Response" and "Chatter".)

Logic Output (Pins 3 and 6)

Output terminals 3 and 6 provide a binary logic output when an input signal tone is present within the detection-band of each respective decoder section. The logic outputs are uncommitted "bare-collector" power transistors capable of switching high current loads. The current level at the output is determined by an external load resistor, R_L, connected from V_{CC} to Pins 3 or 6.

When an in-band signal is present, the output transistor at Pins 3 or 6 saturates with a collector voltage less than 1 volt (typically 0.6V) at full rated current of 100mA. If large output voltage swings are needed, R_L can be connected to a supply voltage, V+ higher than the V_{CC} supply. For safe operation, V+ ≤ 15 volts.

Regulator By-Pass (Pin 12)

This pin corresponds to the output of the voltage regulator section. For circuit operation with a supply voltage greater than 7V, Pin 12 should be ac grounded with a bypass capacitor ≥ 1μF. For circuit operation over a supply voltage range of 4.5 to 7V, the voltage regulator section is not required; Pin 12 should be shorted to V_{CC}.

Ground Terminals (Pins 4 and 5)

To eliminate parasitic interaction, each decoder section has a separate ground terminal. The internal regulator shares a common ground with decoder section A (Pin 4).

Independent ground terminals also allow additional flexibility for split supply operation. Pin 4 can be used as V-, and Pin 5 as ground, as shown in Figure 16. When the circuit is operated with split supplies, the positive supply should always be >6V, and the dc potential across Pins 13 and 14 should not exceed 15 volts.

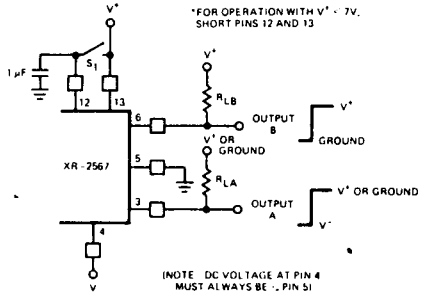


Figure 16. Split-Supply Operation Using Independent Ground Terminals of Units A and B. Unit A Operates Between V+ and V-: Unit B Operates Between V+ and Ground

OPTIONAL CONTROLS

Speed of Response

The minimum lock-up time is inversely related to the loop frequency. As the natural loop frequency is lowered, the turn-on transient becomes greater. Thus, maximum operating speed is obtained when the value of capacitor C_2 is minimum. At the instant an input signal is applied, its phase may drive the oscillator away from the incoming frequency rather than toward it. Under this condition, the lock-up transient is in a worst case situation, and the minimum theoretical lock-up time will not be achievable.

The following expressions yield the values of C_2 and C_3, in microfarads, which allow the maximum operating speeds for various center frequencies. The minimum rate that digital information may be detected without losing information due to turn-on transient or output chatter is about 10 cycles/bit, which corresponds to an information transfer rate of $f_o/10$ baud.

$$C_2 = \frac{130}{f_o}, \quad C_3 = \frac{260}{f_o}$$

In situations where minimum turn-off time is of less importance than fast turn-on, the optional sensitivity adjustment circuit of Figure 17 can be used to bring the quiescent C_3 voltage closer to the threshold voltage. Sensitivity to beat frequencies, noise, and extraneous signals, however, will be increased.

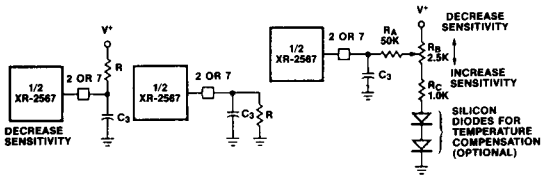


Figure 17. Optional Connections for Sensitivity Control

Chatter

When the value of C_3 is small, the lock transient and ac components at the lock detector output may cause the output stage to move through its threshold more than once, resulting in output chatter.

Although some loads, such as lamps and relays will not respond to chatter, "logic" may interpret chatter as a series of output signals. Chatter can be eliminated by feeding a portion of the output back to the input or, by increasing the size of capacitor C_3. Generally, the feed- back method is preferred since keeping C_3 small will enable faster operation. Three alternate schemes for chatter prevention are shown in Figure 18. Generally, it is only necessary to assure that the feedback time constant does not get so large that it prevents operation at the highest anticipated speed.

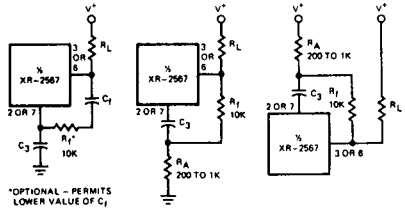


Figure 18. Methods of Reducing Chaffer

Skew Adjustment

The circuits shown in Figure 19 can be used to change the position of the detection band (capture range) within the largest detection band (or lock range). By moving the detection band to either edge of the lock range, input signal variations will expand the detection band in one direction only. Since R_3 also has a slight effect on the duty cycle, this approach may be useful to obtain a precise duty cycle when the circuit is used as an oscillator.

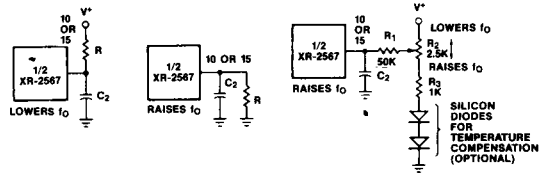


Figure 19. Connections to Reposition Detection Band

Output Latching

After a signal is received, the output of either decoder section can be latched "on" by connecting a 20kΩ resistor and diode from the "output" terminal to the "output filter" terminal as shown in Figure 20. The output stage can be unlatched by raising the voltage level at the output filter terminal.

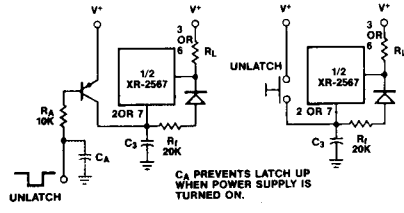
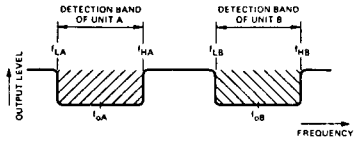


Figure 20. Output Latching

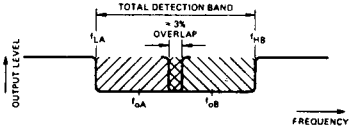
Positioning of Detection Bands

Figure 21 defines the respective band-edge and band-center frequencies for sections A and B of the dual tone decoder.

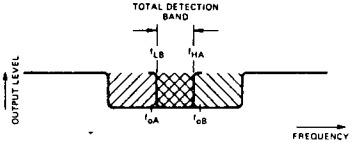
Frequencies f_L and f_H with appropriate subscripts refer to the low and the high band-edge frequencies for decoder sections A and B, and f_o is the center frequency.



(a) Independent Detection of Two Separate Tones



(b) Addition of Detection Bandwidth for Wide-Band Detection



(c) Subtraction of Bandwidths for Narrow-Band Detection

Figure 21. Positioning of Detection Bands

The two sections can be interconnected to form a single tone detector with an overall detection bandwidth equal to the sum or the difference of the detection bands for the two individual detector sections. For example, if the individual decoder sections are interconnected as shown in Figure 25, then the total detection bandwidth would be approximately equal to the sum of the respective bandwidths as shown in Figure 21(b). Similarly, if the decoders are interconnected as shown in Figure 23, then the overall detection band would be equal to the difference, or the overlap, between the respective bandwidths as shown in Figure 21(c).

Bandwidth Reduction

The bandwidth of each decoder can be reduced by either increasing the loop filter capacitor C_2 or reducing the loop gain. Increasing C_2 may be an undesirable solution since this will also reduce the damping of the loop and thus slow the circuit response time.

Figure 22 shows the proper method of reducing the loop gain for reduced bandwidth. This technique will improve damping and permit faster performance under narrow band operation. Bandwidth reduction can also be obtained by subtracting overlapping bandwidths of the two decoder sections (see Figures 21(c) and 23).

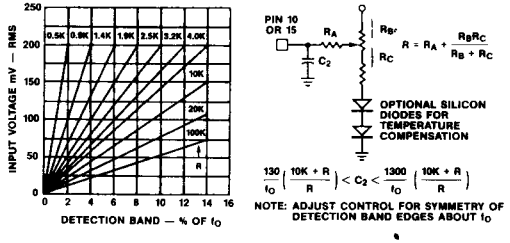


Figure 22. Bandwidth Reduction

APPLICATIONS

Dual-Tone Detection

In most dual-tone detection systems, the decoder output is required to change state only when both input tones are present simultaneously. This can be implemented by setting the detection bandwidth of each of the XR-2567 decoder sections to cover one of the input tones; and then connecting the respective outputs through a NOR gate, as shown in Figure 23. In this case, the output of the NOR gate will be "high" only when both input tones are present simultaneously. Due to capacitor and device variation, it is not possible to use a fixed R1 value in production applications.

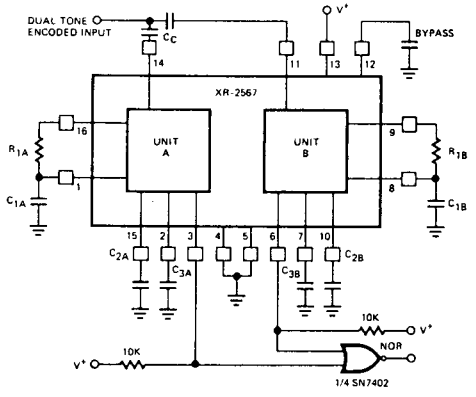


Figure 23. Connection for Decoding Dual-Tone Encoded Input Signals

Figure 24 shows additional circuit configurations which can be used for decoding multiple-tone input signals. In Figure 24(a), the output of Unit A is connected to the output filter (Pin 7) of Unit B through the diode D_1. If no input tone is present within the detection-band of Unit A, then its output (pin 3) is "high", which keeps diode D_1 conducting and "disables" Unit B by keeping its output (pin 6) "high". If an input tone is present within the detection-band of Unit A, Pin 3 is low, diode D_1 is reverse biased, and decoder B is no longer disabled. If under these conditions an input signal is present within the detection-band of Unit B, then its output at Pin 6 would be "low". Thus, the output at Pin 6 is "low" only when input tones within the detection-band of A and B are present simultaneously.

The dual-tone decoder circuit of Figure 24(b) makes use of the split-ground feature of the XR-2567. The output terminal of Unit A is used as a "switch" in series with the ground terminal (Pin 5) of Unit B. If the input tone A is not present, Pin 3 is at its high-impedance state, and the ground terminal of Unit B is open-circuited. When the input tone A is present, Pin 3 goes to a low-impedance state and Unit B is activated. In this manner, the output of Unit B will be "low" only when both tones A and B are present.

In the circuit connection of Figure 24(b), Unit B does not draw any current until it is activated. Therefore, its power dissipation in a stand-by condition is lower than other dual-tone decoder configurations. However, due to finite series resistance between Pin 3 and ground when Unit B is activated, the output current sink capability is limited to ≤ 10mA.

Sequential Tone Decoding

Dual-tone decoder circuits can also be used for sequential tone decoding where one tone must be present before the other for the circuit to operate. This can be achieved by making the output filter capacitance, C_3, of one of the sections large with respect to the other. For example, in the circuits of Figures 24(a) and 24(b), if C_{3A} is chosen to be much larger than C_{3B} ($C_{3A} \geq C_{3B}$), then Unit A will remain "on" and activate B for a finite time duration after tone A is terminated. Thus, the circuit will be able to detect the two tones only if they are present sequentially, with tone A preceding tone B.

The circuit of Figure 24(a) can also be modified for sequential tone decoding by addition of a diode, D_2, between pins 3 and 6. Once activated by Unit A, Unit B will stay "on" as long as tone B is present, even though tone A may terminate. Once tone B disappears, the circuit is reset to its original state and would require tone A to be present for activation.

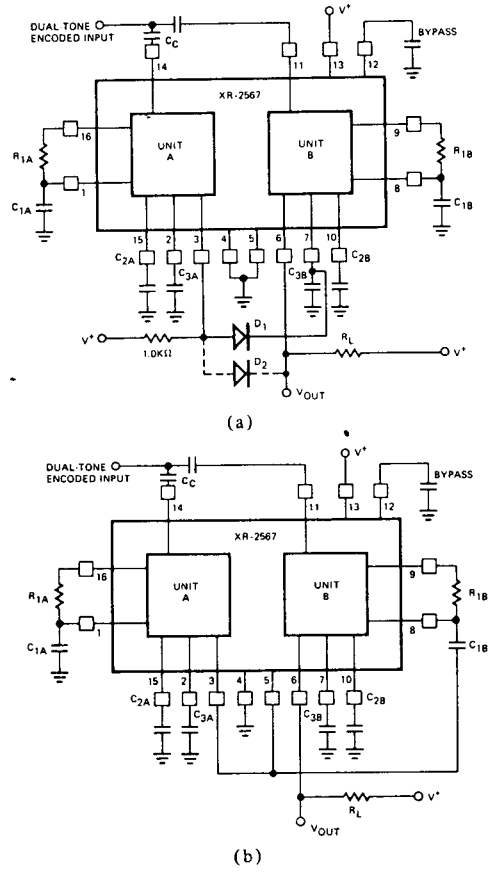


Figure 24. Additional Dual-Tone Decoding Circuits

High-Speed Narrow-Band Tone Decoder

The circuit of Figure 23 can be used as a narrow-band tone decoder by overlapping the detection bands of Units A and B (see Figure 21(c)). The output of the NOR gate will be high only when an input signal is present within the overlapping portions of the detection band. To maintain uniform response within the pass-band, the input signal amplitude should be ≥ 80mV rms. For minimum response time, PPL filter capacitors C_{2A} and C_{2B} should be:

$$C_{2A} = C_{2B} = \frac{130}{f_o\,(Hz)}\ \mu F$$

Under this condition, the worst-case output delay is ≈ 10 to 14 cycles of the input tone.

The practical matching and tracking tolerances of individual units limit the minimum bandwidth to ≈ 4% of f_o.

Wide-Band Tone Decoder

Figure 25 is a circuit configuration for increasing the detection bandwidth of the XR-2567 by combining the respective bandwidths of individual decoder sections. If the detection bands of each section are located adjacent to each other as shown in Figure 21(b), and if the two outputs (pins 3 and 6) are shorted together, then the resulting bandwidth is the sum of individual band-widths. In this manner, the total detection bandwidth can be increased to 24% of center frequency. To maintain uniform response throughout the pass band, the input signal level should be ≥ 80mV, rms, and the respective passbands of each section should have ≈ 3% overlap at center frequency.

Tone Transceiver

The XR-2567 can be used as a full-duplex tone transceiver by using one section of the unit as a tone detector and the remaining section as a tone generator. Since both sections operate independently, the circuit can transmit and receive simultaneously, A recommended circuit connection for transceiver applications is shown in Figure 26. In this case, Unit A is utilized as the receiver, and Unit B is used as the transmitter. The transmitter section can be keyed "on" and "off" by applying a pulse to pin 8 through a disconnect diode D_1. The oscillator section of Unit B will be keyed "off" when the keying logic level at pin 8 is at a "low" state.

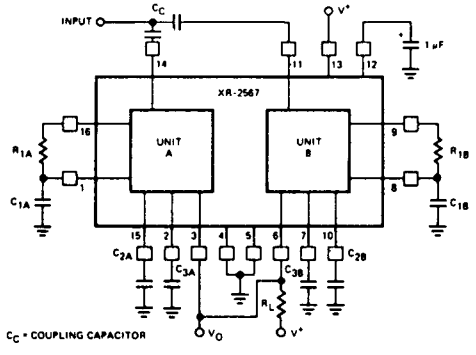


Figure 25. Wide-Band Tone Detection

The output of the transmitter section (Unit B) can also be frequency modulated over a +6% deviation range by applying a modulation signal to pin 10.

High Current Oscillator

The oscillator output of each section of XR-2567 can be amplified using the high current logic driver sections of the circuit. In this manner, each section of the circuit can switch 100mA loads, without sacrificing oscillator stability. A recommended circuit connection for this application is shown in Figure 27. The oscillator frequency can be modulated over 16% of f_o by applying a control voltage to pins 15 or 10.

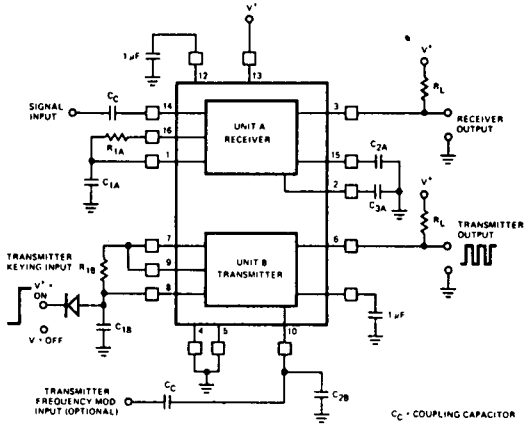


Figure 26. Tone Transceiver

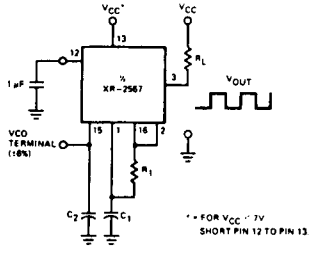


Figure 27. Precision Oscillator with High Current Output Capability